D E S C R I P T I O N

METHOD FOR PRODUCING A SEQUENCE SYNCHRONIZED WITH AN EXTERNAL SIGNAL AND SYNCHRONIZATION CIRCUIT AND RECEIVER

5   **Field of the invention**

The invention relates to a method for producing an internal sequence of analog values having a specific period which corresponds to an external sequence coded in a received signal and is synchronous with it, according to the

10   precharacterizing clause of Claim 1, and also a synchronization circuit for carrying out the method and a receiver comprising at least one said synchronization circuit. Methods of this type serve for decoding specific signals in communication technology, as used in particular

15   in mobile telephony and in positioning systems, such as GPS.

Prior art

In GPS receivers, which are used below as an example, a plurality of signals emitted by satellites have to be assigned to the corresponding satellites and their phase

20   positions accurately determined so that the transit times and hence the distance of the receiver from the satellites can be determined. In each case a digital signal which is based on a specific fundamental sequence of so-called chips which characterizes the satellites, a pseudorandom sequence

25   of length N = 1023, is modulated on the signals having a carrier frequency of 1575.42 MHz by means of phase modulation. The transmission time of the fundamental sequence is 1 ms, and the transmission time of a chip is

therefore the 1023 th part of a millisecond, i.e. slightly less than 1 µs.

The satellite also transmits digital data by logical combination of a data bit value with 20 consecutive copies

5   of the fundamental sequence. Since the transmission of the fundamental sequence takes 1 ms, the data transmission rate is 50 bit/s. The received signal therefore consists in each case of a sequence of repetitions of the 20-fold fundamental sequence, the 20-fold fundamental sequence either being

10 inverted or not, depending on the data bit value. The fundamental sequence is a so-called Gold sequence. The signal is usually very weak and has a large negative signal/noise ratio on the decibel scale.

Various methods have been proposed for identifying the

15 fundamental sequence and determining the phase position of the received signal. Thus, for example, while an external sequence of binary values is derived from the received signal in a high frequency stage, each of the possible fundamental sequences is generated locally in the receiver

20 and in each case copies thereof shifted by various intervals are correlated with the external sequence. In all cases where no agreement is found, the search can be terminated only after checking all possible shifts of the fundamental sequence. Owing to the relatively large length thereof, this

25 is a time-consuming procedure, unless it is performed in a highly parallel manner, which, however, increases both the circuit complexity and hence the costs of the receiver and the energy consumption as well.

According to another method (WO-A-02/25 829), a segment of

30 the external sequence is subjected to a Fourier transformation and is multiplied by the Fourier

transformation of the fundamental sequence, which
transformation is stored in the receiver, and the result is
subjected to inverse transformation. This corresponds to a
convolution of the segment of the external sequence with the
5 fundamental sequence, the resulting values of which in each
case correspond to the correlations of the segment with that
copy of the fundamental sequence which has been time-shifted
by a corresponding number of chips, so that their maximum
indicates the phase position. However, this method too
10 requires considerably complex circuitry and leads to a
relatively high energy consumption in the receiver.

For so-called m-sequences, it is also known (US-A-5 579 337,
US-A-5 612 973, WO-A-01/37 441) that an internal sequence
synchronous with an external sequence can be generated by
15 using an analog feedback shift register which is fed in each
case with an input value which was obtained from a
superposition of a feedback value with the actual value of
the external sequence, which feedback value is generated by
logical combination of older values. However, it has been
20 found that this method cannot be directly applied to other
sequences, such as, for example, Gold sequences. Moreover,
the embodiments of the method which have become known to
date fail in the case of large negative signal/noise ratios,
as are typical in particular for GPS signals.

25   **Summary of the invention**

It is the object of the invention to provide a method of the
generic type which permits, with relatively uncomplicated
circuitry and low energy consumption, rapid and reliable
identification of the fundamental sequence and determination
30 of the phase position of the external signal. This object is

achieved by the features in the characterizing clause of
Claim 1.

It is also intended to provide a synchronization circuit
suitable for carrying out the method and a suitable
5   receiver. These objects are achieved by the features in the
characterizing clause of Claims 17 and 20, respectively.

Brief description of the drawings

Below, the invention is explained in more detail on the
basis of figures which show only an embodiment.

10   Fig. 1   substantially shows a high frequency
                              part of a receiver according to the
                              invention,

     Fig. 2   shows a baseband part of said receiver,

     Fig. 3   shows a component of the baseband part,

15   Fig. 4   shows a synchronization circuit
                              according to the invention,

     Fig. 5   shows the graph of a feedback function
                              used in the method according to the
                              invention,

20   Fig. 6   shows a section of a Gold sequence as
                              coded in the signal of a GPS satellite,

     Fig. 7   shows, on a larger scale, a section from
                              the Gold sequence of Fig. 6,

Fig. 8   shows a section of the signal at the
                            output of the high frequency part, which
                            section corresponds to the section of
                            Fig. 6,

5   Fig. 9, 10   show sections of the signal at specific
                            points of the baseband part, which
                            sections correspond to the section of
                            Fig. 6,

Fig. 11a-c, 12a-c   show sections of the signal at further
10   points of the baseband part, which
                            sections correspond to the section from
                            Fig. 6, and

Fig. 13   shows the development of the power of a
                            feedback signal in the baseband part
15   during synchronization.

Description of the preferred embodiments

The method according to the invention and the
synchronization circuit for carrying it out and the receiver
are described below for a GPS receiver by way of example.
20 Method, synchronization circuit and receiver are, however,
suitable for all applications in which data are transmitted
CDMA-coded and the fundamental sequence of binary values
which is used has the property that it is capable of being
generated by logical combination of two generating binary
25 sequences, at least one of which is a m-sequence or has the
property that it can be generated by a binary feedback shift
register and the phase position of segments of the length of
the shift register can be unambiguously determined in the
fundamental sequence. In addition to Gold sequences, Kasami

6

sequences and others which can be found in the literature
fulfil this condition. For further examples, cf. for example
J.D. Olsen: Nonlinear binary sequences with asymptotically
optimum periodic cross-correlation (Dissertation University
5 of California 1977). The apparatuses described below, with
at most insignificant adaptations, can also be used in an
application well beyond the GPS system.

As mentioned, Gold sequences are used in the GPS system.
They can be generated by logical combination of two so-
10 called preferred pairs of m-sequences. Each m-sequence can
be generated by a binary feedback shift register of length n
and has, inter alia, the property that, with one exception,
each sequence of length n - in the present case, n = 10 -
occurs exactly once in the m-sequence of length $N = 2^n-1$ -
15 in this case 1023 - i.e. the position of such a segment in
the m-sequence can be unambiguously determined.

Various representations are possible for the binary
quantities and their logical combination. Most familiar is
the representation of 0 and 1 with the addition modulo 2
20 (also known as exclusive-or logical combination)
$(b_1,b_2) \rightarrow b_1 \oplus b_2$ as both an associative and a commutative
operation, according to the following table:

$b_2 \backslash b_1$	0	1
0	0	1
1	1	0

The logical combination of an element with the zero element
25 0 leaves the former unchanged, while the logical combination
with 1 converts 0 into 1 and 1 into 0. Since $b \oplus b$ is always
0, the logical combination also has the property that

(1) $(b_1 \oplus b_2) \oplus b_2 = b_1 \oplus 0 = b_1,$

i.e. the logical combination of the result of combining two initial elements with one of the initial elements results in the other initial element.

5   The transformation

(2) $b \rightarrow p = 2b - 1$

leads to the following representation, which is equivalent but more easily implemented and which is used in the embodiment:

$p_2 \backslash p_1$	-1	1
-1	-1	1
1	1	-1

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Here, the logical operation is produced by the mapping

(3) $(p_1, p_2) \rightarrow p_1 \otimes p_2 = -p_1 \cdot p_2.$

-1 is the zero element. The logical operation can evidently be readily extended to include any real numbers, i.e. analog
15 values.

Each m-sequence $p_1, \ldots, p_N$ with $N = 2^n - 1$ can be generated, starting from an initial sequence $p_1, \ldots, p_n$ of length n which does not consist exclusively of zero elements, by recursively forming further values according to the pattern:

20   (4) $p_i = p_{i-n} \otimes p_{i-rm} \otimes \ldots \otimes p_{i-r1},$

where $0 < r_1 < \ldots r_m < n$ and the polynomial $x^n + x^{r_m} + \ldots + x^{r_1} + 1$ is prime with respect to the arithmetic defined above. For example, in each case

(5) $p_i = p_{i-10} \otimes p_{i-3}$

5   may apply. Since all N possible segments of length n, apart from the segment consisting only of zero elements, are passed through before the initial sequence recurs, the choice of the latter is of no importance.

For the formation of a Gold sequence $s_1, \ldots, s_N$, two
10 m-sequences $p_1, \ldots, p_N$ and $q_1, \ldots, q_N$, which form a so-called preferred pair of m-sequences, are used as generating sequences for the Gold sequence, i.e. the Gold sequence is generated from these sequences by element-by-element logical combination:

15 (6) $s_i = p_i \otimes q_i$

Kasami sequences are likewise generated by element-by-element logical combination from two generating sequences, one of which is a m-sequence. For the properties of m-sequences, Gold sequences, Kasami sequences, reference is
20 made to the literature, e.g. E.H. Dinan, B. Jabbari: Spreading Codes for Direct Sequence CDMA and Wideband CDMA Cellular Networks, IEEE Communications Magazine 9/1998, page 48-54.

The GPS receiver shown in Fig. 1-4 and formed according to
25 the invention has a high frequency part (Fig. 1) with an antenna 1 for receiving the signals emitted by the GPS satellites, which is followed by a low-noise self-regulating amplifier 2 and a band-pass filter 3. This is followed by a

first mixer stage comprising a mixer 4, which mixes the
amplified and filtered received signal with a sinewave
signal of 1391.82 MHz which is generated by an oscillator 5,
and a band-pass filter 6 and a second mixer stage

5 fundamentally of the same design and comprising a mixer 7,
which mixes the signal with a sinewave signal of frequency
180.6 MHz which is generated by an oscillator 8, and a band-
pass filter 9. The two mixer stages are finally followed by
an A/D converter 10.

10 In the baseband part (Fig. 2), the signal path branches into
a I path and a Q path, each with a further mixing stage. The
I-path contains a mixer 11 in which the signal is mixed with
a sinewave signal of about 3 MHz which is generated by an
oscillator 12, while the second part contains a further,

15 otherwise identical mixer 13 in which the same signal is
mixed with the sinewave signal of the oscillator 12, which
is phase-shifted by 90° by a phase shifter 14. The mixer 11
is followed by a low-pass filter 15, behind which the path
again branches, and does so to sampling elements 16, 17, to

20 the first one directly and to the second one via a delay
element 18, which delays the signal by a ΔT of about 0.5 μs.
A circuit of exactly the same design is connected to the
mixer 13. The sampling element 16 is followed by a buffer 19
and a further branch. One path leads directly to an output

25 and the other via an inverter 20. A circuit of exactly the
same design is connected to the sampling element 17.
Altogether, the baseband part has 8 outputs, each of which
is connected to the input of a series of separate
synchronization circuits, each of which is assigned to a

30 specific satellite and synchronizes with the fundamental
sequence used by it.

The buffer 19 comprises (Fig. 3) an adder 21 and a shift register 22 having 1023 memory locations for analog values. The output of the shift register 22 is led back to the second input of the adder 21. Each synchronization circuit

5 (Fig. 4) comprises a logic element 23 which follows the input and which is followed by an adder 24, and furthermore an analog feedback shift register 25 having ten memory locations. A feedback circuit 26 is connected with taps at the tenth memory location and at a further memory location

10 or a plurality of further memory locations. In the example, in accordance with (5), only one further tap is present, at the third memory location. In the feedback circuit 26, the tapped analog values are combined according to a feedback function. The graph of a possible feedback function having

15 two arguments $f(x_1, x_2)$ is shown in Fig. 5. The output of the feedback circuit 26 is connected via a gain block 27 to the second input of the adder 24. The adder 24 thus forms a superposition circuit for superposing a feedback value with an intermediate value obtained from the logic element 23.

20 The output of the gain block 27 is also connected to a discriminator 28 which contains a squaring circuit or another circuit mapping the input signal into the positive domain, a low-pass filter and a threshold value detector and outputs a binary signal. The discriminator can also be

25 connected at some other point to the loop formed by the shift register 25, the feedback circuit 26, the gain block 27 and the adder 24. Also provided is a memory 29 to which is fed a determinative set of binary values which is derived from all values stored in the shift register 25 and whose

30 output is connected to the second input of the logic element 23.

Fig. 6 shows a 100 μs section of the fundamental sequence of
the GPS satellite with the ID number 1. This fundamental
sequence is a Gold sequence which can be generated from a
first generating m-sequence $p_1, \ldots, p_{1023}$, which is defined by
5   the feedback according to (5), and a second generating
m-sequence $q_1, \ldots, q_{1023}$. Fig. 7 shows the first 10 μs of the
section of Fig. 6. The fundamental sequence is modulated in
the satellite onto a carrier signal with a frequency of
1575.42 MHz, in such a way that each change of binary value
10 therein is represented by a phase jump of 180° in the
carrier signal.

Of the signals received by the antenna 1 and amplified by
the amplifier 2, substantially the signals originating from
the GPS satellites present in the reception range pass
15 through the band-pass filter 3 into the adjacent mixer
stages, where the carrier frequency is converted down to an
intermediate frequency of 3 MHz. The signal prepared in this
manner and corresponding to the section shown in Fig. 7 is
shown in Fig. 8. The signal is digitized in the A/D
20 converter 10 with a specific bit resolution, e.g. 12 bit for
the magnitude and an additional bit for the sign. The
obtained signal values can be represented as floating point
numbers or as integers. However, they are referred to below
as analog values to distinguish them from binary values. The
25 figures show signals without a background noise, whereas in
fact the very weak signals in the antenna are buried in high
background noise, the typical signal/noise ratio being about
-35 dB.

In the mixers 11 and 12, the signals shown in Fig. 9 and 10
30 are now generated by mixing with sinewave signals of about 3
MHz. The first signal originates from the I-path, i.e. from
mixing of the signal with the sinewave signal generated by

the oscillator 12 in the mixer 11, and the second from the
Q-path, i.e. from mixing with the sinewave signal phase-
shifted by 90° in the mixer 13. The result is a
superposition of the signal coding the fundamental sequence

5   with a sinewave signal whose frequency corresponds to the
sum of the frequencies, i.e. about 6 MHz. The doubling of
the paths is required because, in the case of a phase shift
of the sinewave signal by ± 90° relative to the signal
originating from the A/D converter 10, that component

10   thereof which codes the fundamental sequence would be
cancelled out in the I path. In the present case, since the
phase shift is only 30°, the corresponding component in the
I-path is more pronounced.

The frequency of the oscillator 12 can be controlled. Since

15   the carrier frequency can be Doppler-shifted by a few kHz,
depending on the actual movement of a satellite, a
corresponding frequency range must, for example, be swept
over step by step. For this purpose, the frequency of the
oscillator 12 can be varied in a controlled manner.

20   The signal is now fed into the I- and in the Q-path, in each
case via a low-pass filter 15 which filters out the high-
frequency components, directly to the sampling element 16,
and via the delay element 18, to the sampling element 17. By
means of the delay of the signal by a ΔT of about 0.5 µs,

25   which corresponds to half a chip length, in the delay
element 18, it is ensured that at least one sampling
operation is effected at points in time where the signal is
well defined. Fig. 11a shows the signal of the I-path after
the low-pass filter 15, i.e. before the sampling, Fig. 11b

30   shows the sequence of analog values which the sampling
element 16 generates therefrom and Fig. 11c shows the analog
value at the output of the sampling element 17. Fig. 12a-c

13

show the corresponding signals of the Q-path. In the example, the output signal of the sampling element 16 evidently most clearly reflects the original sequence of Fig. 7. For easier comprehension, in each case only a
5   section of the signal sent by satellite No. 1 is shown in the various stages of processing. In fact, however, in each case a superposition of all received signals is processed in this stage of the receiver.

The corresponding analog values now pass to the buffer 19.
10 There, a plurality, for example, twenty, instances of consecutively determined sequences of in each case 1023 values, each of which corresponds to a fundamental sequence with added background noise - which after all is sent twenty times in succession for transmitting one data bit - are
15 superposed, i.e. the 1023 analog values of the first instance which correspond to the chips of the fundamental sequence are stored in the memory locations of the shift register 22 and then fed back sequentially to the adder 21, and the corresponding values of the second instance are
20 added thereto and the original value is overwritten with the result. This is repeated until the sum of the twenty instances is stored in the shift register 22.

Since, in the summation, the noise is superposed only in an uncorrelated manner, a substantial improvement of the
25 signal/noise ratio can be achieved thereby. If, however, the data bit value changes during the summation and the corresponding fundamental sequence is inverted, the summation can also lead to partial cancellation. In this case, however, no synchronization occurs within a specific
30 time span with regard to this fundamental sequence which then leads to termination and filling of the shift register 22 with new data, as will be explained further below.

The basic sequence stored in the buffer 19 is now read out
repeatedly for generating an external sequence and in each
case fed to the inputs of two synchronization circuits
(Fig. 4), in particular to one directly and to the other via
5   an inverter 20, since the fundamental sequence may be
inverted by logical combination with the data bit.

The various basic sequences stored in the four buffers 19
and derived from analog values $a_1, \ldots, a_{1023}$ derived from the
received signal are now fed, directly and in inverted form,
10   as an external sequence repeatedly to the eight following
instances of the synchronization circuit according to
Fig. 4, which synchronize with the fundamental sequence of
satellite No. 1. An instance which acquires an advantageous
sequence, i.e. one which contains a component as similar as
15   possible to the coded fundamental sequence $s_1, \ldots, s_{1023}$,
should now generate therefrom an internal sequence which
corresponds to the fundamental sequence $s_1, \ldots, s_{1023}$ of
satellite No. 1 and which additionally should agree with the
external sequence with regard to the phase position. This is
20   possible in principle in a satisfactory manner for
m-sequences by means of a synchronization circuit in which a
value which was derived by feedback from the shift register
is superposed with the external sequence and the result is
fed back to the shift register, but not for Gold sequences.

25   In the synchronization circuit according to the invention,
an intermediate signal is therefore first generated by
element-by-element logical combination with a further
sequence, from which intermediate signal the input signal to
the shift register 25 is then obtained. In the synchronized
30   state in which the generated internal sequence of analog
values substantially corresponds to the external sequence,

apart from a noise component, the synchronization circuit functions as follows:

The external sequence corresponds to repetitions of the basic sequence which contains the fundamental sequence

5   $s_1, \ldots, s_{1023}$ with added background noise, said sequence being generated according to (6) by element-by-element logical combination of the first generating m-sequence $p_1, \ldots, p_{1023}$ and of the second generating m-sequence $q_1, \ldots, q_{1023}$. In the synchronized state, the shift register 25 generates the

10   first generating m-sequence. The content of the shift register 25, $a_{i-10}, \ldots, a_{i-1}$, thus corresponds to a segment of this m-sequence, i.e. $p_{i-10}, \ldots, p_{i-1}$ for any i with $1 \leq i \leq 1023$. Since it is a m-sequence, this i can be uniquely determined and hence also the corresponding value q_i of the second

15   generating sequence. This value is read out of the memory 29, which is structured as a table with 1023 memory locations, the sign bits of the values $p_{i-10}, \ldots, p_{i-1}$ being used as a determinative set, which then serves as an address of the table location of q_i.

20   The next element of the external sequence, which, apart from a noise component, substantially corresponds to s_i, is logically combined with q_i in the logic element 23, which, according to (6) in conjunction with (1), substantially gives p_i as an intermediate value. This value is added in

25   the adder 24 to the feedback value from the feedback circuit 26 which is scaled in the gain block 27. However, this latter value likewise corresponds substantially to p_i since it was in fact generated by the feedback, defining the first generating sequence, from the values $a_{i-10}, \ldots, a_{i-1}$

30   corresponding substantially to $p_{i-10}, \ldots, p_{i-1}$, in the specific case by combination of a_{i-10} with a_{i-3}. The superposition of the feedback value with the intermediate value thus

16

corresponds to a_i and is fed as a new input value into the shift register 25. The system is evidently consistent. The sequence of a_i generated in the analog feedback shift register 25 substantially corresponds to repetitions of the

5   first generating m-sequence $p_1,\ldots,p_{1023}$. By element-by-element logical combination with the second generating m-sequence $q_1,\ldots,q_{1023}$, an internal sequence corresponding to repetitions of the fundamental sequence $s_1,\ldots,s_{1023}$ can be generated therefrom.

10 For the stability and the synchronization behaviour in the case of the large negative signal/noise ratios prevailing in GPS receivers, the choice of a suitable feedback function f is of considerable importance. With the functions known to date, it has not been possible to achieve synchronization in

15 the case of sequences with a high background noise. In the search for more suitable feedback functions, various features have proved to be advantageous. Thus, in the case of the chosen representation of the binary values - in the case of other representations, the properties must in some

20 cases be appropriately transformed - it should as far as possible have the following properties:

If the magnitudes of the arguments are 1, the magnitude of the feedback value should be slightly less than 1, preferably between 0.90 and 0.99. It is advantageous if, in

25 the case of arguments of magnitude 1, the feedback function gives a value of magnitude 1, i.e.

(7) $\left| f(x_1,\ldots,x_m) \right| = 1$ for $\left| x_1 \right| = \ldots = \left| x_m \right| = 1,$

and the function value is then multiplied by a selectable factor $k<1$, in particular $0.90<k<0.99$. This multiplication

is performed by the adjustable gain block 27, which follows
the feedback circuit 26 evaluating the feedback function.

The sign of the feedback function should in each case be the
inverse of the sign of the product of the negative
5   arguments, i.e.

(8) $sig(f(x_1,\ldots,x_m)) = -sig((-x_1) \cdot \ldots \cdot (-x_m))$.

If $x_1,\ldots,x_m$ each have the magnitude 1, i.e. can also be
regarded as binary quantities, said two properties result in
$f(x_1,\ldots,x_m)$ corresponding to the logical combination
10 $x_1 \otimes \ldots \otimes x_m$.

It is furthermore advantageous if the feedback function f is
invariant on interchanging the arguments. It should be
antisymmetrical and monotonic as a function of each
individual argument, i.e. when other arguments are kept
15 constant.

It has proved to be particularly advantageous if the
feedback function in each sector which is defined by
specific values of the signs of the arguments is
substantially a linear combination of the arguments. The
20 resulting discontinuities at the sector limits can be
smoothed, but it has been found that such modifications tend
to have an adverse effect on the behaviour and therefore
should not be large. A feedback function f which has all the
above-mentioned properties and with which it was possible to
25 achieve synchronization even in the case of signals with
high background noise is

(9) $f(x_1,\ldots,x_m) = -sig((-x_1) \cdot \ldots \cdot (-x_m)) \cdot (|x_1|+\ldots+|x_m|)/m$

18

Apart from scaling which ensures that (7) is satisfied, this function is in each sector a linear combination of the arguments with coefficients of +1 or -1.

For two variables, i.e.

5   (10) $f(x_1, x_2) = -sig(x_1 \cdot x_2) \cdot (|x_1| + |x_2|)/2,$

it is shown in Fig. 5, only the transitions at the sector limits having been smoothed by linear interpolation.

Since the synchronization circuit operates with stored data, its operating speed is independent of the chip rate of the
10 received signal and can be substantially higher. The power of the internal sequence generated, which is taken off at the output of the gain block 27, serves as a criterion for successful synchronization. While the elements of the internal sequence have about the same value as those of the
15 external sequence before synchronization, the latter sequence is amplified by a factor 1/(1-k), which is thus usually between 10 and 100, when synchronization is complete. The power of the internal sequence $(a_1)_{i=1,\ldots,1023}$ accordingly increases sharply, as shown in Fig. 13. This
20 increase is registered by the discriminator 28, in which the power is determined by squaring and smoothed by filtering through a low-pass filter and averaged over a relatively long time segment, and finally the result is compared with a threshold value. It outputs a corresponding binary signal
25 which indicates that synchronization is complete.

If no synchronization occurs after a specific time, there is in general no sense in continuing the procedure with the same data. The absence of synchronization may be accidental, for example due to a particularly unfavourable form of the

noise component, due to an unfavourable phase position of
the received signal or due to an unfavourable sampling time
before a data bit change, which results in the addition, in
the buffers 19 (Fig. 2) of instances of sequences in which
5   the component containing the desired fundamental sequence
occurs with different signs, which can lead to a serious
attenuation of said component compared with the noise
component. In such cases, it is expedient to fill the
buffers 19 with new basic sequences and to begin the
10   synchronization process again with them.

Up to 32 satellites whose fundamental sequences differ are
in use in the GPS system. Since it is intended to employ the
signals of all satellites in the receiving range, the
receiver should in each case contain types of
15   synchronization circuits corresponding to all satellites in
use, each type synchronizing with the fundamental sequence
of one of the satellites. The types differ in memory
content, which determines the second generating m-sequence
$q_1, \ldots, q_{1023}$. Instead of being located at the end of the
20   baseband part, where 32 different synchronization circuits
can be connected to each output, the branching to the
various types can also be located further to the front in
the signal path, e.g. at the end of the high frequency part.
This has the advantage that, for example, the frequency of
25   the oscillator 12 can be set more specifically to the
trajectory of the respective satellite with utilization of
further information. On the other hand, multiple
implementation of the entire baseband part is of course
required.

30   The example described can of course be modified in many
ways. Thus, for example, intermediate frequencies other than
those mentioned can be chosen or some or all of the

intermediate stages can be omitted. Various possibilities
are also available for implementing the synchronization
circuit and the receiver; in particular different degrees of
integration can be chosen. The shift registers can, for
5   example, each be formed by a corresponding memory with
linear addressing and a write pointer and a read pointer.

List of reference symbols

     1   Antenna
     2   Amplifier
10   3   Band-pass filter
     4   Mixer
     5   Oscillator
     6   Band-pass filter
     7   Mixer
15   8   Oscillator
     9   Band-pass filter
     10   A/D converter
     11   Mixer
     12   Oscillator
20   13   Mixer
     14   Phase shifter
     15   Low-pass filter
     16   Sampling element
     17   Sampling element
25   18   Delay element
     19   Buffer
     20   Inverter
     21   Adder
     22   Shift register
30   23   Logic element
     24   Adder
     25   Shift register

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26 Feedback circuit

27 Gain block

28 Discriminator

29 Memory

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